A Novel Tunable Comline Bandpass Filter Based on External Quality Factor and Internal Coupling Tunings

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Abstract — A combline filter with quasi-elliptic performance with external quality factor and internal coupling tuning is presented in this paper. In this design, a wide center frequency tuning range with a constant 3-dB FBW (fractional bandwidth) and ABW (absolute bandwidth) is obtained. Also, it is demonstrated that the transmission zero located at the lower edge of passband can be adjusted with little effect on the passband characteristic. A prototype of the tunable filter with a tuning range of 1.27GHz to 2.25GHz is fabricated on a substrate with ε=10.2 and h=1.27mm. Through tuning internal coupling coefficient and external quality factor, one can make the filter operate over a wide center frequency tuning range, with a constant 3-dB FBW (fractional bandwidth) nearly kept at 54% or ABW (absolute bandwidth) nearly kept at 500 MHz.

Index Terms—Absolute bandwidth, coupling coefficient, fractional bandwidth, quality factor, tunable filter, transmission zero.

I. INTRODUCTION

Tunable bandpass filter is increasingly concerned in recent years, which is available to reduce the overall size and complexity of the modern communication and radar systems. Compared with other tunable filters, the combline topology is most frequently applied in the circuit design, due to its several advantages, such as miniaturization, one unique transmission zero in the upper band, convenience for integration and so on [1-9]. In [1-2], the designed method on the basis of the detailed formulas for a fundamental combline bandpass filter is presented, also its application is discussed. In [3-4], the resonator of SIR is utilized to keep the absolute bandwidth constant during the center frequency tuning. In [5], the short-circuited end of the resonator applied in combline filter is replaced by the lumped series resonator. And a wide tuning range can be achieved with only a small capacitance ratio of varactor. In [6], two coupled lines are introduced between the adjacent resonators to produce the source/load coupling and the multi resonator coupling. Then five tunable transmission zeros are created at the upper passband. In [7], the series RC unit is added to the first and last resonator to make the Q factor distribution of the resonator non-uniform. And then the passband flatness and selectivity of the filter are enhanced. In [8-9], the tunable filter with constant fractional bandwidth and absolute bandwidth is designed. Due to the cross coupling mechanism of the combline filter, transmission zeroes is always produced only at the upper passband edge, thus improving the selectivity of the filter at one side. However, the smoothing decrease of the rejection at the lower passband limits its practical application. Thus, another new transmission zero should be created at the lower passband to tackle the problem.

Several tunable combline filters with elliptic function performance have been designed [10-12]. In [10], a three-pole combline filter with two tunable transmission zeros located at two edges of the passband is presented. The additional transmission zero at the lower side is created due to a section line shunted with a varactor. In [11], a cross coupling between the non-adjacent resonators is produced, thus a new transmission zero is supposed to be generated to give the filter a quasi-elliptic performance. It is noted that [12] firstly demonstrates a four-pole combline filter with a pair of tunable transmission zeros at the two edges. And the phase difference between the main transmission path and other paths is analyzed to explain the production of the zeros. However, although some improvement is made to the performance of combline filter, how to simultaneously adjust the external quality factor and the internal coupling coefficient to control the bandwidth and control the position of the novel transmission zero is not discussed.

In this paper, a novel combline bandpass filter in Fig. 1 is presented. Varactors are employed to connect the adjacent resonators, the resonator and the I/O coupling
transmission line to tune the external quality factor and internal coupling tuning together. Therefore, the relative bandwidth and absolute bandwidth can be adjusted during the center frequency tuning, and in the paper FBW or ABW is nearly invariable in the process of the center frequency change. In addition, the application of a novel transmission line which produces the cross coupling between the I/O transmission lines creates a novel tunable transmission zero at the lower passband edge, thus, improving the selectivity of the designed filter. In this way, the tunable filter with fixed bandwidth can be used to connect with frequency synthesizer (PLL or DDS) which produces frequency-hopping signal of constant power, several blocking capacitors are utilized. What’s more, a cross coupling path are introduced here to bring additional transmission zero at lower passband. And, the characteristic impedances of the two microstrip lines at the input/output ports are both 50Ω.

In Fig. 1, the circuit configuration of the proposed tunable filter is shown. It can be seen that thirteen varactors marked as $D_1$, $D_2$, $D_3$, and $D_4$ are applied to satisfy the requirement for center frequency, internal coupling coefficient, external $Q$ factor and the transmission zero tuning. Besides, to provide the DC power, several blocking capacitors $C$ are utilized. What’s more, a cross coupling path are introduced here to bring an additional transmission zero at lower passband. And, the characteristic impedances of the two microstrip lines at the input/output ports are both 50Ω.

It is clear from Fig. 1 that the varactor $D_3$ is applied to change the external $Q$ factor of the filter, while $D_3$ used to tune the internal coupling coefficient. And the technique to calculate the $Q$ factor and coupling coefficient can be found in [13-14]. Hence, Fig. 2 (a) is drawn to present the relationship between the $Q$ factor and capacitance value of $D_3$, while the coupling coefficient vs. capacitance value of $D_3$ is given in Fig. 2 (b). In the figures, four capacitance values of $D_1$ that controls center frequency are considered. As is known, $Q=g_{01}g_{10}/FBW$ and $M_{i,i+1}=FBW/(g_{i+1})$. Thus, various combination of $Q$ and $M_{i,i+1}$ means different bandwidth. Taking $D_1=1.2\,\text{pF}$ as an example, 52.3% of $FBW$ which is the final result in this paper will be obtained when making $D_2$ and $D_4$ equal $1.1\,\text{pF}$ and $1.3\,\text{pF}$.

![Fig. 1. Circuit of proposed tunable combline bandpass filter](image)

**II. ANALYSIS AND DESIGN OF THE PROPOSED TUNABLE FILTER**

In Fig. 1, the circuit configuration of the proposed tunable filter is shown. It can be seen that thirteen varactors marked as $D_1$, $D_2$, $D_3$, and $D_4$ are applied to satisfy the requirement for center frequency, internal coupling coefficient, external $Q$ factor and the transmission zero tuning. Besides, to provide the DC power, several blocking capacitors $C$ are utilized. What’s more, a cross coupling path are introduced here to bring an additional transmission zero at lower passband. And, the characteristic impedances of the two microstrip lines at the input/output ports are both 50Ω.

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filter around 1.26GHz, while $D_2$ and $D_3$ which respectively determine the external $Q$ factor and internal coupling coefficient are equal to 3.2pF and 4pF. $D_4$ deciding the position of novel transmission zero is assigned 7.1pF on the basis of the technique involved below. And from Fig. 2 (d), with the decrease of the value of $D_1$, one should correspondingly reduce the values of $D_2$ and $D_3$ simultaneously to fix the $FBW$ depending on Fig. 2 (a) and Fig. 2 (b). And, properly adjusting the values of $D_2$ and $D_3$, $FBW$ can be almost unchanged in the whole process of center frequency tuning. What’s more, it is seen from Fig. 2 (e) that properly adjusting $D_2$ and $D_3$ simultaneously, the absolute bandwidth ($ABW$) can also be almost unchanged during the $D_4$ change. To maintain a constant $ABW$ during the increase of center frequency, the coupling coefficient should be decreased and the external quality increased.

For the conventional combine tunable filter, one transmission zero is always created at the upper passband edge, thus improving the selectivity of the filter at one side. So, another transmission zero should be produced at the lower passband to improve the rejection. In this paper, an additional signal propagation path whose equivalent circuit model is shown in Fig. 3 (a) is introduced from input coupling line to the output one. Hence, the quasi-elliptic performance is expected because of the multiple path cancellation. And the location of novel transmission zero is decided by the resonating frequency of the coupled lines.

Figure 3 (b) and Fig. 3 (c) show the odd mode and the even mode equivalent circuit. It is obvious from Fig. 3 (c) that even mode resonating frequency is non-adjustable. In this case, the odd mode resonating frequency which can be controlled by $D_4$ is used to adjust the novel transmission zero. $S_{11o}$ of the odd mode equivalent circuit in Fig. 3 (b) can be written as $S_{11o}=(Y_{22o}+Y_{oo})(Y_{11}+Y_{ino}),$ where $Y_0$ is the characteristic admittance of the circuit, $Y_{ino}=(-Y_{11}\times Y_{22o}+Y_{12o}^2)/(Y_{12o}Y_{11}),$ where $Y_{11}$, $Y_{22}$ and $Y_{12}$ can be found as below:

$Y_{11} = Y_{22} = -j0.5(Y_{ee} + Y_{oo})\cot(\theta),$  

$Y_{12} = Y_{21} = -j0.5(Y_{eo} - Y_{oo})\csc(\theta),$  

$Y_{oo} = j(Y_{oo}C + Y_{ao}^2\tan(\theta))/(Y_{ee} - \sigma C\tan(\theta)).$  

In the equations, $Y_{ee}$ and $Y_{oo}$ denote the even mode characteristic impedance and the odd mode characteristic impedance of the coupling line, $\theta = \theta = \theta_0.$ And the odd mode resonating frequency which makes $S_{11o}=0$ true, identifies the location of transmission zero. And, the equivalent circuit simulation in ADS (Advanced Design System) also indicates the resonating frequency of odd mode and even mode. In addition, Fig. 3 (d) is presented to demonstrate how the value of $D_4$ influences the resonating frequency.
how the produced transmission zero is controlled by $D_4$, Fig. 3 (e) and Fig. 3 (f) are given. And, the proper value should be set to $D_2$ and $D_3$ based on Fig. 2 (a) and Fig. 2 (b). What is shown in Fig. 3 has proven that adjustment of $D_4$ results in the change of the transmission zero at lower band. However, as the novel transmission zero moved away from the passband, a resonating transmission pole becomes increasingly obvious. Hence, to tackle the problem, the value of $D_4$ is chosen carefully to make the lower transmission zero approach passband.

III. DESIGN OF THE TUNABLE FILTER

Based on the analysis above, the design parameters are determined as follows:

Step 1): Select the third-order low-pass prototype with elements. Then calculate the external quality factors $Q_e$ and the coupling coefficient $M_i$ through $Q_e=g_{0i}/FBW$ and $M_{i+1}=FBW/(g_{i+1}g_{i})$, where $FBW$ is the 3-dB fractional bandwidth.

Step 2): Determine the dimensions of the proposed tunable resonator. Initially, the impedance of the transmission line is conveniently selected as 72Ω ($W_f=0.5\text{mm}$ is chosen initially), and the electrical length of the coupled line is set to 45 degrees at 1.7GHz ($L=7.4\text{mm}$), according to the required frequency tuning range. The spacing $S_{12}$ between two resonators can then be determined. An initial value for $S_{12}$ is chosen such that the coupling coefficient of the coupled resonators satisfies the bandwidth requirement at the center frequency.

Step 3): The rest of the design parameters are then determined. The coupling I/O structure is adopted to satisfy the constant bandwidth requirement over a wide tuning range because it has wideband matching behavior. The input/output line is typically chosen to be a high impedance line for tight coupling; $S_{01}$ and $W_0$ are then chosen to satisfy external quality factors $Q_e$, using the well-known coupling coefficient/external $Q_e$ method described in [13].

Step 4): An additional signal propagation path shown in Fig. 3 (a) is employed from input coupling line to the output one to create a novel transmission zero. And equivalent circuit technique is adopted to find the initial value of $S_c$ and $L_c$. In the paper, short coupling lines of 15 degrees in length are chosen. And $S_c$ is selected to be the same as $S_{12}$ for simplicity.

Step 5): Finally, some necessary optimization is carried out, making use of electromagnetic EM simulation in SONNET. The estimated circuit dimensions from previous steps are substituted into a full wave EM simulator for including discontinuity, via-hole, and non-adjacent coupling effects. And when the center frequency is changed by $D_1$, another group of value for $D_2$, $D_3$ and $D_4$ units must be updated to keep the good passband performance based on Fig. 2 and Fig. 3.

A tunable filter of constant bandwidth is designed
on RT/Duroid 6010 with $\varepsilon_r=10.2$ and $h=1.27$mm with an overall size of 22×25mm². Electro-magnetic simulation software of SONNET is applied for the optimization. Three kinds of silicon junction varactor diodes produced by Nanjing Electronic Devices Institute are applied. WB62 ($C_i=0.45-4.23pF; R_s=1\Omega; Q=3000$ at 50MHz for $C_i=1.07pF$) is selected as $D_1$ to accomplish the center frequency tuning, while the wide tuning range varactor WB2011H ($C_i=1.79-20.53pF; R_s=0.5\Omega; Q=1200$ at 50MHz for $C_i=6.73pF$) is chosen to adjust the location of the transmission zero. Besides, for the trivial space between the two adjacent resonators, the bondable chip varactor W205 ($C_i=0.8-11.54pF; R_s=1.2\Omega; Q=800$ at 50 MHz for $C_i=3.55pF$) is considered as the candidate for the coupling coefficient and external $Q$ factor control, and the bonding wire is applied to finish the connection. Murata 0402 lumped components and 100pF chip capacitors are used for DC blocking and biasing.

Fig. 4. Photography of the tunable combline filter.

In Fig. 4, the photography of the novel tunable filter is introduced. And the simulation and measured result in which the bandwidth is nearly kept unchanged are given in Fig. 5 and Fig. 6. The filter with the lowest center frequency 1.27GHz is optimized at the beginning ($D_1=3.4pF, D_2=3.2pF, D_3=4.3pF, D_4=7pF$). Then, $D_1$ is decreased to raise the center frequency to be 2.25GHz, while $D_4$ is reduced to move up the transmission zero correspondingly according to Fig. 3. Finally, $D_2$ and $D_3$ are adjusted monotonously to be 1pF and 0.6pF to keep a constant quality factor and coupling coefficient. Thus, nearly a constant fractional bandwidth can be acquired. And, for the case with unchanged absolute bandwidth during center frequency moving, $D_2$ and $D_3$ are tuned to be 1.2pF and 3.5pF.

According to [10], the following equation indicates that $FBW$ and $Q_u$, both mainly determine the insert loss of the filter:

$$IL(dB) = 4.343 \sum g_i \Delta Q_i$$

where $\Delta$ stands for the fractional bandwidth and $Q_u$ represents the unloaded quality factor of resonator. Again, $g_0=g_1=1$, $g_2=1.2275$ and $g_3=1.1525$ for Chebyshev lowpass prototype filters are considered and $Q_u$ of the resonator covers the value range of 50 to 90 during center frequency tuning. Thus, $IL$ is almost less than 2dB for most tuning cases. However, the measured insertion loss at the tuning range varies from 3dB to 5dB. This difference of $IL$ is due to the SMA connector and the deviation of the diode’s index.

Figure 5 and Fig. 6 demonstrate the simulated and measured results, with the center frequency turning from 1.27GHz to 2.25GHz. One can figure out that the filter achieves the quasi-elliptic performance. And the adjustment of $D_4$ makes the transmission zero close to the passband. Besides, $D_2$ and $D_3$ are changed correspondingly during center frequency tuning in order to keep the $FBW$ and $ABW$ invariant. As a result, the range of 52.5%–55.8% of the fractional bandwidth and absolute bandwidth of 490MHz–512MHz are obtained. To see the similarity, both the simulated and measured curves are plotted in one graph as shown in Fig. 5 and Fig. 6. Good agreement can be observed between the simulated and the experimental results. The slight frequency shift and difference of insert loss between measured and simulated results may be caused by the fabrication errors and the SMA connector. So, the comparing results given below have proven the advantage of the novel structure.

Fig. 5. Simulated and measured results of combline filter with constant $FBW$. (Voltage for the varactors during measurement is turning as below: $V_1$:5.1-0.9V; $V_2$:11.3-1.9V; $V_3$:17.6-2.9V; $V_4$:19.4-3.1V).

The comparisons of measured results for several tunable filters [5, 10-12] are shown in Table 1. It can be concluded that although the capacitance ratio for $D_1$ in this paper is not the smallest one, the tuning range of the
center frequency is wider than other compared structures. And as other tunable filters, the one introduced in the paper also have two transmission zeros at passband edges to improve the rejection. And the lower transmission zero can even be adjusted. Finally, being different from other tunable filters, FBW can almost be invariant during center frequency changing for the designed one in the paper.

Fig. 6. Simulated and measured results of combline filter with constant ABW. (Voltage for the varactors during measurement is turning as below: V;:5.1–0.9V; V2:11.7-2.1V; V3:9.2–1.6V; V4:19.4-3.1V).

### Table 1: Comparisons with wideband filters

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### IV. CONCLUSION

In this work, a 1.27–2.25GHz tunable combline bandpass filter based on external quality factor and internal coupling tuning is proposed. During the tuning of the center frequency, coupling coefficient and external quality factor are adjusted to keep the bandwidth as a constant value. Additionally, a novel transmission line is applied to generate the coupling between the I/O transmission lines to produce a new tunable transmission zero at the lower passband edge. Moreover, the quasi-elliptic performance can be observed at the simulation and measurement results. Therefore, the proposed filter exhibits good frequency selectivity, suggesting a good substitute for radio communication application.

### REFERENCES

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